A New Design Approach for Asymmetric Coupled-Section Marchand Balun

Ji An Park · Choon Sik Cho · Jae Wook Lee

Abstract

A systematic design for asymmetric coupled-section Marchand baluns is presented. Asymmetrically coupled transmission lines in multilayer configuration are exploited for constructing Marchand baluns. Design equations for characteristic impedance and electrical length of asymmetrical coupled transmission lines are derived for establishing a systematic design procedure. Novel Marchand balun based on these design equations is composed of two identical asymmetrical coupled transmission lines. However, contrary to the general conventional design approach where ranges for characteristic impedances of coupled lines are ambiguously capitalized, values for characteristic impedance and length are explicitly expressed. Our approach is fundamentally different from the design method using coupling coefficients where solution for coupling coefficient is inherently restricted. To verify the proposed method, one design example is performed for wideband Marchand balun in multilayer configuration, and is fabricated for verifying the design procedure proposed. Maintaining the return loss more than 10 dB, the bandwidth is measured from 0.43 to 1.0 GHz, where $S_{21}$ and $S_{31}$ show better than $-4$ dB. The measured phase and amplitude imbalances illustrate 0.5 dB and $\pm 5^\circ$, respectively.

Key Words: Asymmetric Balun, Asymmetric Coupled Transmission Lines, Marchand Balun, Wideband.

1. INTRODUCTION

Due to compact configuration and ease of fabrication, the Marchand balun has been widely used since it was introduced [1–3]. As the operating frequencies for microwave and millimeter-wave systems increase, baluns composed of transmission lines have been integrated with amplifiers, mixers and frequency generators/converters since the balanced operation takes advantages over single-ended operation on various performances, such as noise reduction, power supply stability, and linearity, etc. [4–6]. MMICs are also now integrating this transmission line based baluns with active and passive circuits in single chip because transmission lines can be integrated conveniently for millimeter-wave frequencies. Therefore, more compact designs for baluns are continuously required for modern microwave and millimeter-wave systems.

The Marchand balun has attracted substantial interest for performing this functionality because this balun can be constructed for very wideband and simple fabrication [7–10]. It is constituted generally using two identical symmetric coupled sections for simplifying the design. Since the symmetric coupled section is mainly characterized by the coupling factor, most of Marchand baluns composed of symmetric coupled sections are established using the design equation for the coupling factor according to design specifications [11–15]. In spite of its relatively easy implementation, Marchand baluns using symmetric coupled sections impose restriction on band extension and adjustability because very tight coupling is needed for wideband and not easy for fabrication. Asymmetric coupled-sections possibly using multilayer con-
figuration may be employed for overcoming this restriction, however the design procedure will be more complicated compared with simple symmetric coupled section based Marchand baluns [16–18].

Not depending upon the coupling coefficient, Marchand balun can also be designed using the procedure presented in [8] where several sets of design equations are derived and capitalized for designing the asymmetric coupled line based Marchand balun. Although [4] and [19] do not use the coupling coefficient, explicit expression for obtaining the design equations are not shown, but just providing available ranges for characteristic impedances of transmission lines located over multilayers. Therefore, it seems to be quite difficult to obtain the exact design parameters, leading to possibility to distracted design since the only ranges for design parameters are given. It is highly desired that the design equations for obtaining circuit configuration be explicitly characterized and the design procedure be clearly defined for asymmetric coupled line based Marchand balun.

In this work, a systematic design for achieving the characteristics of asymmetric coupled transmission lines over two layers is proposed for building the Marchand baluns. We do not use coupling coefficients for the asymmetric coupled lines, instead explicit expression for characteristic impedances is derived. Without using coupling coefficients, characteristic impedance of a transmission line on top layer over wide transmission line located on bottom layer is derived using the balun requirements. The characteristic impedance of the transmission line on bottom layer can also be calculated assuming that this transmission line is so wide that this can be approximated to a single transmission line with ground layer located below this wide line. Other than characteristic impedances, electrical lengths for the coupled lines are also exploited for design parameters, which is not a general procedure for conventional design for Marchand baluns. In conventional design, electrical length is maintained to be 90°, however, electrical length can be varied for achieving the design specifications in this work, specially related to extending the bandwidth. Newly derived design equations are revealed in Section II, a Marchand balun is designed and evaluated according to the proposed procedure as explained in Section III, and finally conclusion is included in Section IV.

II. DESIGN PROCEDURE

The basic Marchand balun can be represented by using transmission lines as shown in Fig. 1(a) where unbalanced signal enters from A and balanced signal comes out between B and C. This type of balun can be equalized to the circuit as shown in Fig. 1(b) where two coupled sections are exploited for obtaining 3-dB insertion loss and coupling factor \( k \) determines the physical dimensions of the coupled sections.

For symmetric coupled sections, even- and odd-mode characteristic impedances are discovered, however, 3-dB coupling providing an overall 3-dB insertion loss for the coupled sections is so tight that this configuration shows a difficulty in obtaining acceptable insertion loss. Relative signal strengths coming into the unbalanced port and out of the balanced port are represented as in Eq. (1) where \( k \) is the coupling factor. As described in Eq. (1), only one solution is available for the coupling factor to achieve zero return loss and 3-dB insertion loss, and in some cases unrealistic physical geometry is required.

\[
Unbalanced = \frac{1-3k^2}{1+k^2} \\
Balanced+ = j\frac{2k\sqrt{1-k^2}}{1+k^2} \\
Balanced- = -j\frac{2k\sqrt{1-k^2}}{1+k^2}
\]

(1)

\[
Z_{ab} > 2Z_a \geq R > Z_b
\]

(2)

Due to this restriction, asymmetric coupled-sections over two layers may replace the symmetric coupled sections for realistic implementation of 3-dB insertion loss. Ambiguous design equation expressed in Eq. (2) has been needed conventionally for obtaining physical geometry of asymmetric coupled-sections as derived in [10]. However, Eq. (2) does
not have to be satisfied if the proposed design approach here in this paper is capitalized as explained later. Since no design equations manifest themselves in explicit expression up to now, it is highly desirable that more obvious representation be derived.

The equivalent circuit for Fig. 1 looking into $Z$ may be redrawn as shown in Fig. 2 where the original unbalanced port can be thought to be propagated back by amount of $\theta_s$ from $Z$ [3]. Since the characteristics of balun can be understood mainly in terms of reflection coefficient at the unbalanced port (port 1) and transmission coefficients from unbalanced port to balanced port, three-port $[S]$-matrix is given as shown in Eq. (3),

$$
[S]_{balun} = \begin{bmatrix}
0 & e^{j\theta} / \sqrt{2} & -e^{-j\theta} / \sqrt{2} \\
e^{-j\theta} / \sqrt{2} & e^{j2\theta} / \sqrt{2} & e^{-j2\theta} / \sqrt{2} \\
e^{-j\theta} / \sqrt{2} & e^{-j2\theta} / \sqrt{2} & e^{j2\theta} / \sqrt{2}
\end{bmatrix}
$$

(3)

To derive the explicit design equations for asymmetric coupled-line based Marchand balun, necessary $S$-parameters for the equivalent circuit as described in Fig. 2 are calculated for balun to work as represented in Eqs. (4)–(6) using $a = j2Z_{ab} \tan \theta_{ab} - jZ_0 \cot \theta_b$, and $b = -jZ_0 \cot \theta_b$,

$$
S_{11} = \frac{(a - Z_0)(b^2 + 2bZ_0 + Z_0^2) - 2b(b^2 + bZ_0)}{\Delta}
$$

(4)

$$
S_{21} = S_{12} = \frac{b^3 + b(-b^2 + bZ_0 + ab + Z_0^2 + aZ_0) - (b^2 + bZ_0)(a - Z_0)}{\Delta}
$$

(5)

$$
S_{31} = S_{13} = \frac{-b^3 - b(-b^2 + bZ_0 + ab + Z_0^2 + aZ_0) + (b^2 + bZ_0)(a - Z_0)}{\Delta}
$$

(6)

where $\Delta = -2b^3 - bZ_0 + ab^2 + 2bZ_0^2 + 2abZ_0 + Z_0^3 + aZ_0^2$.

From Eq. (3), $S_{11}$ should be zero for this equivalent circuit to work as a balun, therefore real and imaginary parts of $S_{11}$ are zero as deduced in Eqs. (7) and (8). Solving Eqs. (7) and (8), two explicit solutions are derived as seen in Eqs. (9) and (10).

$$
Re(S_{11}) = -4Z_{ab}Z_0 \tan \theta_{ab} + 2Z_0Z_{ab}Z_0 \tan \theta_{ab} \cot \theta_b + 3Z_{ab}Z_0 \tan \theta_{ab} - Z_0^3 = 0
$$

(7)

$$
Im(S_{11}) = Z_{ab}^2Z_0 \tan \theta_{ab} \cot \theta_b - Z_0Z_{ab}^2 \cot \theta_b = 0
$$

(8)

$$
Z_0^2 = Z_{ab}^2 \tan \theta_{ab}
$$

(9)

$$
Z_0 \cot \theta_b = Z_{ab} \tan \theta_{ab}.
$$

(10)

Substituting Eqs. (9) and (10) into Eqs. (5) and (6), we can confirm that this equivalent circuit satisfies the requirement for balun to work since $S_{21} = \frac{1}{\sqrt{2}} e^{j225^\circ}$ and $S_{31} = \frac{1}{\sqrt{2}} e^{j45^\circ}$ leading to $|S_{21}| = |S_{31}| = \frac{1}{\sqrt{2}}$ and $\angle S_{21} - \angle S_{31} = 180^\circ$. Once $Z_b$, $Z_{ab}$, $\theta_b$, and $\theta_{ab}$ are determined satisfying Eqs. (9) and (10), physical geometry for balun can be obtained using electromagnetic (EM) simulation programs. $Z_s$ and $\theta_s$ do not affect balun equation, so that they can be equalized to $Z_b$ and $\theta_b$, respectively. Since four parameters are to be determined ($Z_b$, $Z_{ab}$, $\theta_b$, and $\theta_{ab}$), two design freedoms for determining these parameters using Eqs. (9) and (10) are available. Rearranging Eqs. (9) and (10),

$$
Z_0 = \pm Z_s \cot \theta_b = \pm Z_{ab} \tan \theta_{ab}.
$$

(11)

where $90^\circ$ for $\theta_b$ and $\theta_{ab}$ is excluded to determine $Z_b$ and $Z_{ab}$. In case of $90^\circ$ both for $\theta_b$ and $\theta_{ab}$, the capacitance is shorted and inductances are open, resulting in $S_{11}$ of 1/3 (= –9.5 dB). For $Z_0 = Z_b = Z_{ab}$, the perfect match occurs when $\theta_b = \theta_{ab} = 45^\circ$, $135^\circ$, $225^\circ$, etc., as drawn in Fig. 3 where the fractional bandwidth based on $S_{11}$ of under –10 dB goes up to 116%. But for $Z_0$ or $Z_{ab} = Z_b$, $\theta_b$ and $\theta_{ab}$ do not need to be same any more, yielding smaller ba-
For a maximum bandwidth, $\theta_b$ and $\theta_{ab}$ should be maintained close to 90º.

Once $Z_b$ and $Z_{ab}$ are determined initially by considering physical implementation, $\theta_b$ and $\theta_{ab}$ can be determined as close as possible to 90º by taking into account the desired bandwidth in terms of $S_{11}$.

A systematic procedure for designing asymmetric coupled-line based Marchand balun is summarized in the flow diagram of Fig. 4 where two steps are used for arriving at the final physical geometry. The first step, coupled section parameters are decided using Eqs. (9) and (10) from the desired balun specifications. These parameters constitute an equivalent circuit model as in Fig. 2, and S-parameters are calculated for verifying the coupled section parameters. At the second step, the calculated coupled section parameters are exploited to obtain the physical widths and lengths ($W_a$, $W_b$, $W_{ab}$, $l_a$, $l_b$, and $l_{ab}$) as exhibited in Fig. 4. Usually, $W_a$ is set equal to $W_b$, and $l_a = l_b$ is used for simplifying the design. Extended lines with 50 ohms are added to line $l_{ab}$ to connect ports 2 and 3 conveniently to this balun. $W_a$ (= $W_b$) is obtained by regarding the wide transmission line located on bottom layer used as the reference layer, and $W_{ab}$ is obtained as a general transmission line located over a ground layer where narrow transmission line located on top layer is used for synthesizing $W_{ab}$.

The characteristic impedance ($Z_{ab}$) of wide line on bottom layer can be thought to be little deviated from that of a general transmission line since a very narrow line is located on top layer. Therefore, this assumption does not affect the characteristic impedance of wide transmission line on bottom layer.

## III. DESIGN OF THE ASYMMETRIC MARCHAND BALUNS

Based on the design procedure developed in Section II, a balun using asymmetric coupled-sections over two layers is designed varying characteristic impedances as illustrated in Fig. 5. Desired specifications are chosen as listed in Table 1. Design parameters and physical geometries for the design example are achieved as illustrated in Table 2 where the electrical lengths ($\theta_a$ and $\theta_b$) are initially set to 90º at the center frequency of 0.9 GHz as a design freedom. Using Figs. 2 and 3, $\theta_a = 75º$ and $\theta_b = 105º$ are then optimized with the pre-selected $Z_b = 75$ Ω and $Z_{ab} = 33$ Ω. It is found

### Table 1. Desired balun specifications

<table>
<thead>
<tr>
<th>Center frequency ($f_0$)</th>
<th>Bandwidth</th>
<th>$Z_0$</th>
</tr>
</thead>
<tbody>
<tr>
<td>0.9 GHz</td>
<td>&gt; 50%</td>
<td>50 Ω</td>
</tr>
</tbody>
</table>

### Table 2. Parameters for design example of asymmetric coupled-section based balun

<table>
<thead>
<tr>
<th>Parameter</th>
<th>Value</th>
</tr>
</thead>
<tbody>
<tr>
<td>$Z_a$</td>
<td>75 Ω</td>
</tr>
<tr>
<td>$Z_b$</td>
<td>75 Ω</td>
</tr>
<tr>
<td>$Z_{ab}$</td>
<td>33 Ω</td>
</tr>
<tr>
<td>$W_a$</td>
<td>4.6 mm</td>
</tr>
<tr>
<td>$W_b$</td>
<td>4.6 mm</td>
</tr>
<tr>
<td>$W_{ab}$</td>
<td>8.15 mm</td>
</tr>
<tr>
<td>$L_a$</td>
<td>65 mm (75º at $f_0$)</td>
</tr>
<tr>
<td>$L_{ab}$</td>
<td>85 mm (105º at $f_0$)</td>
</tr>
</tbody>
</table>

![Fig. 5. The physical layout of asymmetric coupled-section based Marchand balun.](image)
that the relation between characteristic impedances is completely different from Eq. (2), therefore, a large number of freedoms in choosing design parameters are available.

Using the physical geometry obtained here, an asymmetric coupled-section based Marchand balun has been simulated on a full-wave EM simulator. $S$-parameters obtained from an EM simulator are displayed as shown in Fig. 6, and compared with those calculated from the equivalent circuit model as in Fig. 2. It is seen that the insertion loss is $-3.2$ to $-2.5$ dB, the amplitude imbalance is within $1.5$ dB, and the phase imbalance is less than $5^\circ$ over the frequency range of 0.5 to 1.0 GHz where $|S_{11}|$ is less than $-10$ dB. Although $S_{11}$ obtained from an EM simulator shows disagreement in the higher frequency, $S_{21}$ and $S_{31}$ exhibit considerably outstanding result.
The proposed balun using the layout depicted in Fig. 5 has been fabricated on Duroid 5880 substrate with dielectric constant of 2.2 and each layer thickness of 1.57 mm in two layer structure as shown in Fig. 6. Fig. 7 demonstrates S-parameter results from equivalent model and EM simulation. Deviation at the upper band is originated from the fact that \( Z_a \) and \( Z_b \) used 75 \( \Omega \), resulting in some reflection with 50 \( \Omega \) input (\( = Z_0 \)). Their S-parameters are measured and plotted in Fig. 8. \( |S_11| \) is less than –10 dB over the frequency range of 0.43 to 1.0 GHz. The insertion losses are measured as –3.9 to –3.2 dB as in Fig. 8, the amplitude imbalances are measured less than 0.5 dB, and the phase imbalances are within 5º as shown in Figs. 9 and 10 (within vertically dashed lines), respectively. If 3-dB bandwidth is taken in terms of \( S_{21} \) and \( S_{31} \), the bandwidth is extended to 0.38 to 1.4 GHz range which is around 1 GHz bandwidth. These measurement results are in fairly good agreement with EM simulation results. Two factors affected the frequency response of this balun: 1) since the difference of \( S_{21} \) and \( S_{31} \) seen at port 1 is 0.2 (= –14 dB) at 0.9 GHz when \( Z \) is matched to 75 \( \Omega \), and \( S_{11} \) deviates away from this value as frequency goes up; 2) since the difference of \( L_{ab} \) and \( L_a \) (or \( L_b \)) exists leading to significant effect at the high frequency, this yields degradation of \( S_{11} \) at higher frequency as shown in Figs. 8–10.

The air gap between top and bottom layers has been fabricated and assembled to be kept very little. We watched measured performance by changing the intensity of tightening screws at the corners, but not much difference has been come up with.

### IV. SUMMARY

A design approach for the asymmetric coupled-section based Marchand balun has been presented along with design equations. An equivalent circuit model is exploited for evaluating the initial balun design before synthesizing the physical layout. The analytical procedure provides explicit relation between characteristic impedances of couples sections instead of using coupling factor which has been widely used conventionally. Physical geometry for coupled section is achieved by synthesizing the characteristic impedance of coupled line through an EM simulator.

This approach was validated by taking a design example for asymmetric coupled-section based Marchand balun. This balun was designed using two layers where unbalanced port is located on top layer, balanced port is located on bottom layer, and ground is underneath the bottom layer. One design was fabricated and measured to confirm the proposed design approach. Experimental results are compared with those from an EM simulator where both show good agreement as desired.

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### REFERENCES


Ji An Park received the B.S degree in telecommunication and computer engineering from Korea Aerospace University, Goyang, Korea, in 2014, where he is working toward the M.S. degree in telecommunication and computer engineering. His research interests focus on CMOS radio-frequency front-end circuit and passive circuit design.

Choon Sik Cho received his B.S. in Control and Instrumentation Engineering from Seoul National University in 1987, his M.S. in Electrical and Computer Engineering from the University of South Carolina in 1995, and his Ph.D. in Electrical and Computer Engineering from the University of Colorado in 1998. From 1987 to 1993, he was with LG Electronics, working on communication systems. From 1999 to 2003, he was with Curitel, where he was principally involved with the development of mobile phones. He joined the School of Electronics, Telecommunication and Computer Engineering, Korea Aerospace University, Korea, where he is currently a Professor. His research interests include high power amplifier design, computational electromagnetics, EMI/EMC analysis on PCB, and component design in microwave and millimeterwave.

Jae Wook Lee received the B.S. degree in electronics engineering from Hanyang University, Seoul, Korea, and the M.S. and Ph.D. degrees in electrical engineering (with an emphasis in electromagnetics) from Korea Advanced Institute of Science and Technology (KAIST), Daejeon, Korea, in 1992, 1994, and 1998, respectively. From 1998 to 2004, he was a senior member in the Advanced Radio Technology Department, Radio and Broadcasting Research Laboratory, Electronics and Telecommunications Research Institute (ETRI), Daejeon. He later joined the School of Electronics, Telecommunications and Computer Engineering, Korea Aerospace University, Korea, where he is currently a Professor. His research interests include high power amplifier design, computational electromagnetics, EMI/EMC analysis on PCB, and component design in microwave and millimeterwave.